



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

Absolute Maximum Ratings⁽¹⁾⁽²⁾⁽³⁾

ESD Tolerance ⁽⁴⁾	2.0 kV
Differential Input Voltage	±Supply Voltage
Voltage at Input/Output Pin	(V ⁺) + 0.3V, (V ⁻) - 0.3V
Supply Voltage (V ⁺ - V ⁻)	16V
Current at Input Pin ⁽⁵⁾	±5 mA
Current at Output Pin ⁽⁶⁾⁽⁷⁾	±30 mA
Current at Power Supply Pin	40 mA
Lead Temp. (Soldering, 10 sec.)	260°C
Storage Temperature Range	-65°C to +150°C
Junction Temperature ⁽⁸⁾	150°C

- (1) Absolute Maximum Ratings indicate limits beyond which damage to the device may occur. Operating Ratings indicate conditions for which the device is intended to be functional, but specific performance is not ensured. For ensured specifications and the test conditions, see the Electrical Characteristics.
- (2) For specified Military Temperature Range parameters see RETSMC6462/4X.
- (3) If Military/Aerospace specified devices are required, please contact the Texas Instruments Sales Office/Distributors for availability and specifications.
- (4) Human body model, 1.5 kΩ in series with 100 pF. All pins rated per method 3015.6 of MIL-STD-883. This is a class 2 device rating.
- (5) Limiting input pin current is only necessary for input voltages that exceed absolute maximum input voltage ratings.
- (6) Applies to both single supply and split-supply operation. Continuous short circuit operation at elevated ambient temperature can result in exceeding the maximum allowed junction temperature of 150°C. Output currents in excess of ±30 mA over long term may adversely affect reliability.
- (7) Do not short circuit output to V⁺, when V⁺ is greater than 13V or reliability will be adversely affected.
- (8) The maximum power dissipation is a function of T_{J(MAX)}, θ_{JA}, and T_A. The maximum allowable power dissipation at any ambient temperature is P_D = (T_{J(MAX)} - T_A)/θ_{JA}. All numbers apply for packages soldered directly into a PC board.

Operating Ratings

Supply Voltage	3.0V ≤ V ⁺ ≤ 15.5V	
Junction Temperature Range	LMC6462AM, LMC6464AM	-55°C ≤ T _J ≤ +125°C
	LMC6462AI, LMC6464AI	-40°C ≤ T _J ≤ +85°C
	LMC6462BI, LMC6464BI	-40°C ≤ T _J ≤ +85°C
Thermal Resistance (θ _{JA})	P Package, 8-Pin PDIP	115°C/W
	D Package, 8-Pin SOIC	193°C/W
	NFF Package, 14-Pin PDIP	81°C/W
	D Package, 14-Pin SOIC	126°C/W

- (1) Absolute Maximum Ratings indicate limits beyond which damage to the device may occur. Operating Ratings indicate conditions for which the device is intended to be functional, but specific performance is not ensured. For ensured specifications and the test conditions, see the Electrical Characteristics.

5V DC Electrical Characteristics

Unless otherwise specified, all limits ensured for T_J = 25°C, V⁺ = 5V, V⁻ = 0V, V_{CM} = V_O = V⁺/2 and R_L > 1M. **Boldface** limits apply at the temperature extremes.

Symbol	Parameter	Conditions	Typ ⁽¹⁾	LMC6462AI LMC6464AI Limit ⁽²⁾	LMC6462BI LMC6464BI Limit ⁽²⁾	LMC6462AM LMC6464AM Limit ⁽²⁾	Units
V _{OS}	Input Offset Voltage		0.25	0.5 1.2	3.0 3.7	0.5 1.5	mV max
TCV _{OS}	Input Offset Voltage Average Drift		1.5				µV/°C
I _B	Input Current	See ⁽³⁾	0.15	10	10	200	pA max

- (1) Typical Values represent the most likely parametric norm.
- (2) All limits are specified by testing or statistical analysis.
- (3) Specified limits are dictated by tester limitations and not device performance. Actual performance is reflected in the typical value.

5V DC Electrical Characteristics (continued)

Unless otherwise specified, all limits ensured for $T_J = 25^\circ\text{C}$, $V^+ = 5\text{V}$, $V^- = 0\text{V}$, $V_{\text{CM}} = V_O = V^+/2$ and $R_L > 1\text{M}$. **Boldface** limits apply at the temperature extremes.

Symbol	Parameter	Conditions	Typ ⁽¹⁾	LMC6462AI LMC6464AI Limit ⁽²⁾	LMC6462BI LMC6464BI Limit ⁽²⁾	LMC6462AM LMC6464AM Limit ⁽²⁾	Units
I_{OS}	Input Offset Current	See ⁽³⁾	0.075	5	5	100	pA max
C_{IN}	Common-Mode Input Capacitance		3				pF
R_{IN}	Input Resistance		>10				Tera Ω
CMRR	Common Mode Rejection Ratio	$0\text{V} \leq V_{\text{CM}} \leq 15.0\text{V}$, $V^+ = 15\text{V}$	85	70 67	65 62	70 65	dB min
		$0\text{V} \leq V_{\text{CM}} \leq 5.0\text{V}$ $V^+ = 5\text{V}$	85	70 67	65 62	70 65	
+PSRR	Positive Power Supply Rejection Ratio	$5\text{V} \leq V^+ \leq 15\text{V}$, $V^- = 0\text{V}$, $V_O = 2.5\text{V}$	85	70 67	65 62	70 65	dB min
-PSRR	Negative Power Supply Rejection Ratio	$-5\text{V} \leq V^- \leq -15\text{V}$, $V^+ = 0\text{V}$, $V_O = -2.5\text{V}$	85	70 67	65 62	70 65	dB min
V_{CM}	Input Common-Mode Voltage Range	$V^+ = 5\text{V}$ For CMRR ≥ 50 dB	-0.2	-0.10 0.00	-0.10 0.00	-0.10 0.00	V max
			5.30	5.25 5.00	5.25 5.00	5.25 5.00	V min
		$V^+ = 15\text{V}$ For CMRR ≥ 50 dB	-0.2	-0.15 0.00	-0.15 0.00	-0.15 0.00	V max
			15.30	15.25 15.00	15.25 15.00	15.25 15.00	V min
A_V	Large Signal Voltage Gain	$R_L = 100\text{ k}\Omega$ ⁽⁴⁾	Sourcing	3000			V/mV min
			Sinking	400			V/mV min
		$R_L = 25\text{ k}\Omega$ ⁽⁴⁾	Sourcing	2500			V/mV min
			Sinking	200			V/mV min
V_O	Output Swing	$V^+ = 5\text{V}$ $R_L = 100\text{ k}\Omega$ to $V^+/2$	4.995	4.990 4.980	4.950 4.925	4.990 4.970	V min
			0.005	0.010 0.020	0.050 0.075	0.010 0.030	V max
		$V^+ = 5\text{V}$ $R_L = 25\text{ k}\Omega$ to $V^+/2$	4.990	4.975 4.965	4.950 4.850	4.975 4.955	V min
			0.010	0.020 0.035	0.050 0.150	0.020 0.045	V max
		$V^+ = 15\text{V}$ $R_L = 100\text{ k}\Omega$ to $V^+/2$	14.990	14.975 14.965	14.950 14.925	14.975 14.955	V min
			0.010	0.025 0.035	0.050 0.075	0.025 0.050	V max
		$V^+ = 15\text{V}$ $R_L = 25\text{ k}\Omega$ to $V^+/2$	14.965	14.900 14.850	14.850 14.800	14.900 14.800	V min
			0.025	0.050 0.150	0.100 0.200	0.050 0.200	V max

(4) $V^+ = 15\text{V}$, $V_{\text{CM}} = 7.5\text{V}$ and R_L connected to 7.5V . For Sourcing tests, $7.5\text{V} \leq V_O \leq 11.5\text{V}$. For Sinking tests, $3.5\text{V} \leq V_O \leq 7.5\text{V}$.

5V DC Electrical Characteristics (continued)

Unless otherwise specified, all limits ensured for $T_J = 25^\circ\text{C}$, $V^+ = 5\text{V}$, $V^- = 0\text{V}$, $V_{CM} = V_O = V^+/2$ and $R_L > 1\text{M}$. **Boldface** limits apply at the temperature extremes.

Symbol	Parameter	Conditions	Typ ⁽¹⁾	LMC6462AI LMC6464AI Limit ⁽²⁾	LMC6462BI LMC6464BI Limit ⁽²⁾	LMC6462AM LMC6464AM Limit ⁽²⁾	Units
I _{SC}	Output Short Circuit Current V ⁺ = 5V	Sourcing, V _O = 0V	27	19 15	19 15	19 15	mA min
		Sinking, V _O = 5V	27	22 17	22 17	22 17	mA min
I _{SC}	Output Short Circuit Current V ⁺ = 15V	Sourcing, V _O = 0V	38	24 17	24 17	24 17	mA min
		Sinking, V _O = 12V ⁽⁵⁾	75	55 45	55 45	55 45	mA min
I _S	Supply Current	Dual, LMC6462 V ⁺ = +5V, V _O = V ⁺ /2	40	55 70	55 70	55 75	μA max
		Quad, LMC6464 V ⁺ = +5V, V _O = V ⁺ /2	80	110 140	110 140	110 150	μA max
		Dual, LMC6462 V ⁺ = +15V, V _O = V ⁺ /2	50	60 70	60 70	60 75	μA max
		Quad, LMC6464 V ⁺ = +15V, V _O = V ⁺ /2	90	120 140	120 140	120 150	μA max

(5) Do not short circuit output to V⁺, when V⁺ is greater than 13V or reliability will be adversely affected.

5V AC Electrical Characteristics

Unless otherwise specified, all limits ensured for $T_J = 25^\circ\text{C}$, $V^+ = 5\text{V}$, $V^- = 0\text{V}$, $V_{CM} = V_O = V^+/2$ and $R_L > 1\text{M}$. **Boldface** limits apply at the temperature extremes.

Symbol	Parameter	Conditions	Typ ⁽¹⁾	LMC6462AI LMC6464AI Limit ⁽²⁾	LMC6462BI LMC6464BI Limit ⁽²⁾	LMC6462AM LMC6464AM Limit ⁽²⁾	Units
SR	Slew Rate	See ⁽³⁾	28	15 8	15 8	15 8	V/ms min
GBW	Gain-Bandwidth Product	V ⁺ = 15V	50				kHz
φ _m	Phase Margin		50				Deg
G _m	Gain Margin		15				dB
	Amp-to-Amp Isolation	See ⁽⁴⁾	130				dB
e _n	Input-Referred Voltage Noise	f = 1 kHz V _{CM} = 1V	80				nV/√Hz
i _n	Input-Referred Current Noise	f = 1 kHz	0.03				pA/√Hz

(1) Typical Values represent the most likely parametric norm.

(2) All limits are specified by testing or statistical analysis.

(3) V⁺ = 15V. Connected as Voltage Follower with 10V step input. Number specified is the slower of either the positive or negative slew rates.

(4) Input referred, V⁺ = 15V and R_L = 100 kΩ connected to 7.5V. Each amp excited in turn with 1 kHz to produce V_O = 12 V_{PP}.

3V DC Electrical Characteristics

Unless otherwise specified, all limits ensured for $T_J = 25^\circ\text{C}$, $V^+ = 3\text{V}$, $V^- = 0\text{V}$, $V_{\text{CM}} = V_O = V^+/2$ and $R_L > 1\text{M}$. **Boldface** limits apply at the temperature extremes.

Symbol	Parameter	Conditions	Typ ⁽¹⁾	LMC6462AI LMC6464AI Limit ⁽²⁾	LMC6462BI LMC6464BI Limit ⁽²⁾	LMC6462AM LMC6464AM Limit ⁽²⁾	Units
V_{OS}	Input Offset Voltage		0.9	2.0 2.7	3.0 3.7	2.0 3.0	mV max
TCV_{OS}	Input Offset Voltage Average Drift		2.0				$\mu\text{V}/^\circ\text{C}$
I_B	Input Current	See ⁽³⁾	0.15	10	10	200	μA
I_{OS}	Input Offset Current	See ⁽³⁾	0.075	5	5	100	μA
CMRR	Common Mode Rejection Ratio	$0\text{V} \leq V_{\text{CM}} \leq 3\text{V}$	74	60	60	60	dB min
PSRR	Power Supply Rejection Ratio	$3\text{V} \leq V^+ \leq 15\text{V}$, $V^- = 0\text{V}$	80	60	60	60	dB min
V_{CM}	Input Common-Mode Voltage Range	For CMRR ≥ 50 dB	-0.10	0.0	0.0	0.0	V max
			3.0	3.0	3.0	3.0	V min
V_O	Output Swing	$R_L = 25\text{ k}\Omega$ to $V^+/2$	2.95	2.9	2.9	2.9	V min
			0.15	0.1	0.1	0.1	V max
I_S	Supply Current	Dual, LMC6462 $V_O = V^+/2$	40	55 70	55 70	55 70	μA
		Quad, LMC6464 $V_O = V^+/2$	80	110 140	110 140	110 140	μA max

(1) Typical Values represent the most likely parametric norm.

(2) All limits are specified by testing or statistical analysis.

(3) Specified limits are dictated by tester limitations and not device performance. Actual performance is reflected in the typical value.

3V AC Electrical Characteristics

Unless otherwise specified, $V^+ = 3\text{V}$, $V^- = 0\text{V}$, $V_{\text{CM}} = V_O = V^+/2$ and $R_L > 1\text{M}$. **Boldface** limits apply at the temperature extremes.

Symbol	Parameter	Conditions	Typ ⁽¹⁾	LMC6462AI LMC6464AI Limit ⁽²⁾	LMC6462BI LMC6464BI Limit ⁽²⁾	LMC6462AM LMC6464AM Limit ⁽²⁾	Units
SR	Slew Rate	See ⁽³⁾	23				V/ms
GBW	Gain-Bandwidth Product		50				kHz

(1) Typical Values represent the most likely parametric norm.

(2) All limits are specified by testing or statistical analysis.

(3) Connected as Voltage Follower with 2V step input. Number specified is the slower of either the positive or negative slew rates.

Typical Performance Characteristics

$V_S = +5V$, Single Supply, $T_A = 25^\circ C$ unless otherwise specified

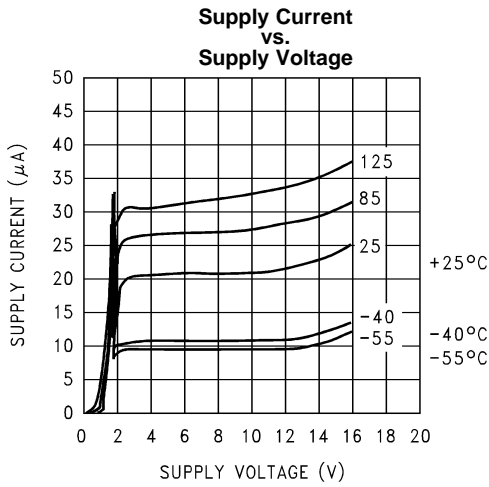


Figure 4.

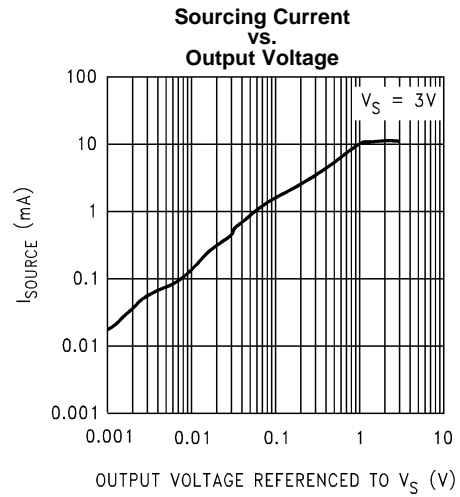


Figure 5.

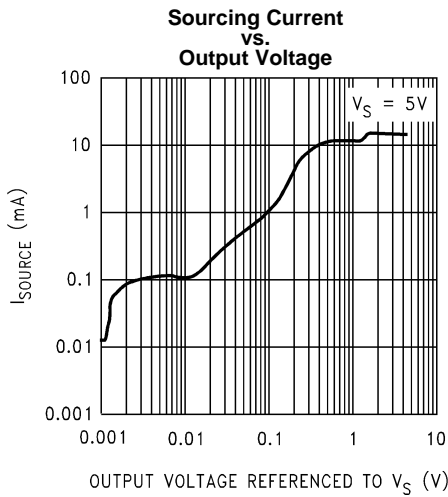


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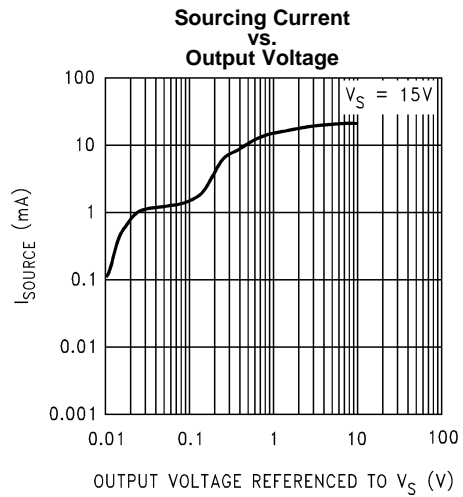


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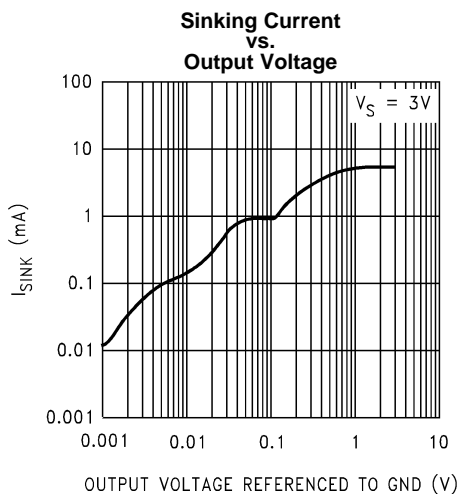


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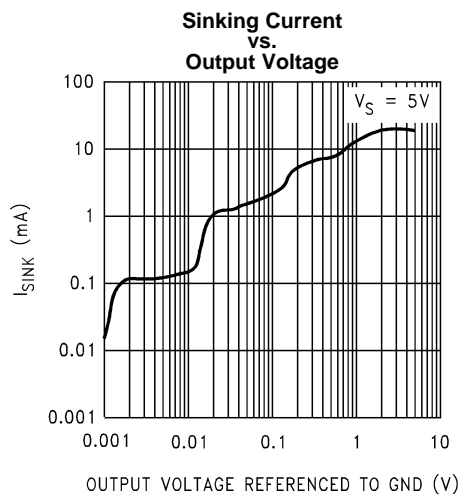


Figure 9.

Typical Performance Characteristics (continued)

$V_S = +5V$, Single Supply, $T_A = 25^\circ C$ unless otherwise specified

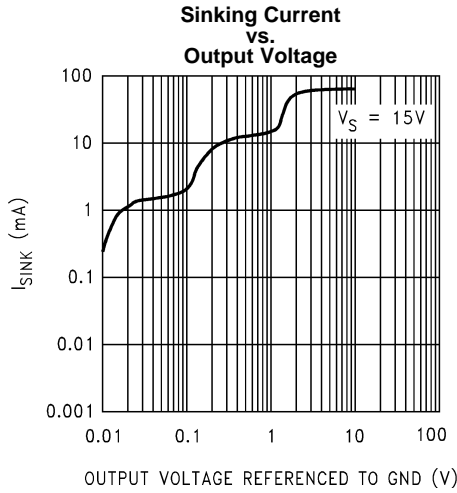


Figure 10.

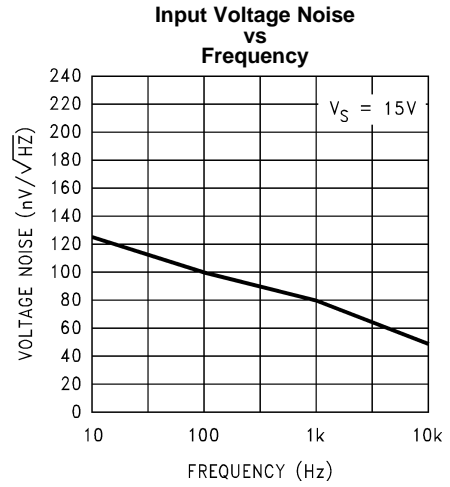


Figure 11.

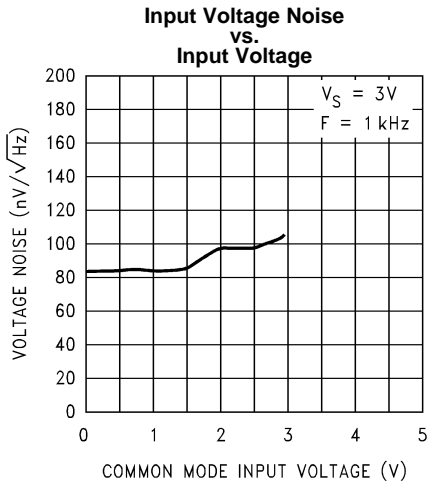


Figure 12.

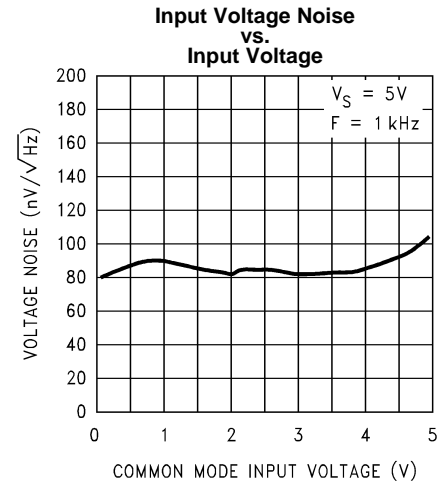


Figure 13.

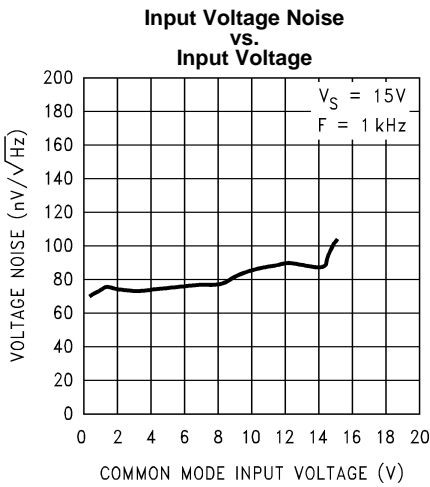


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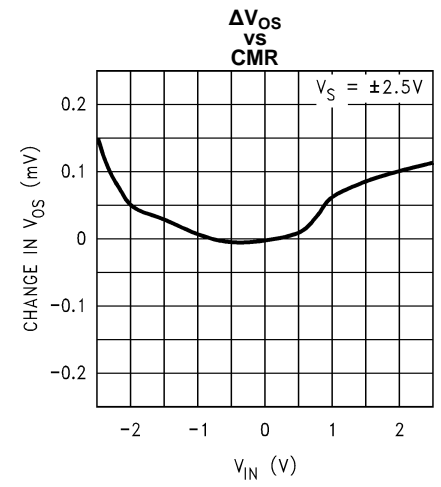


Figure 15.

Typical Performance Characteristics (continued)

$V_S = +5V$, Single Supply, $T_A = 25^\circ C$ unless otherwise specified

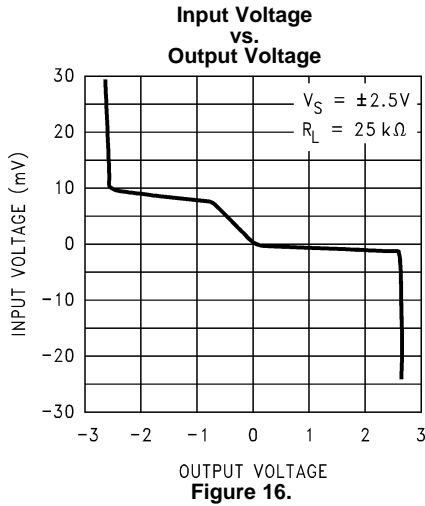


Figure 16.

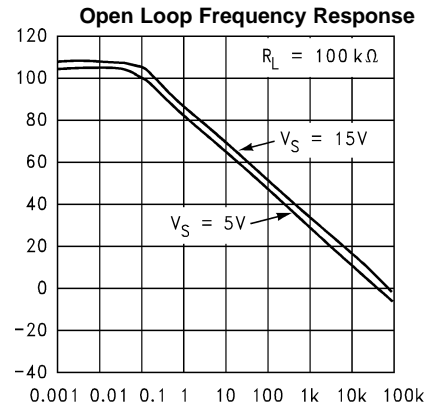


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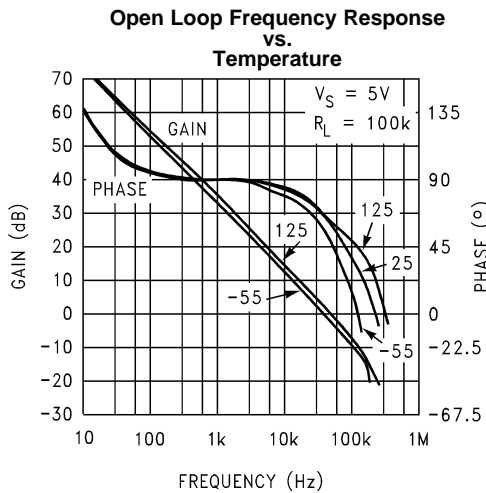


Figure 18.

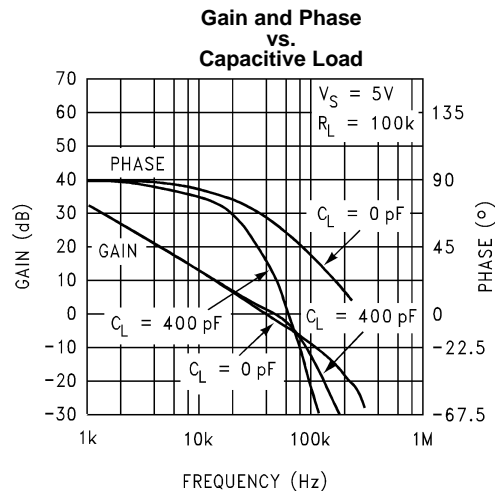


Figure 19.

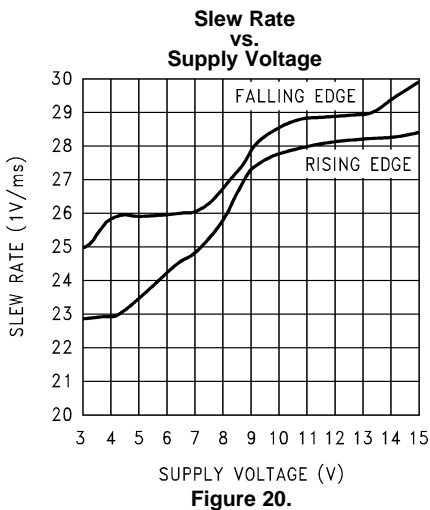


Figure 20.

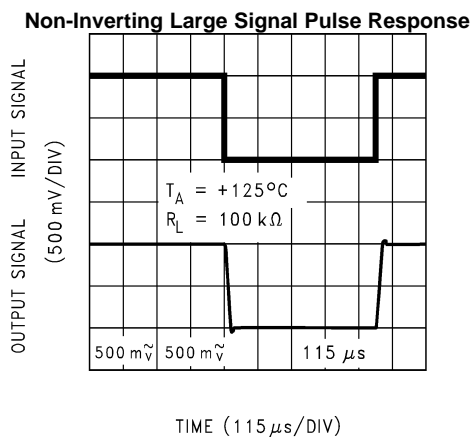
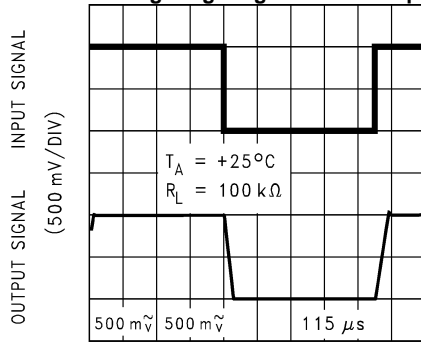


Figure 21.

Typical Performance Characteristics (continued)

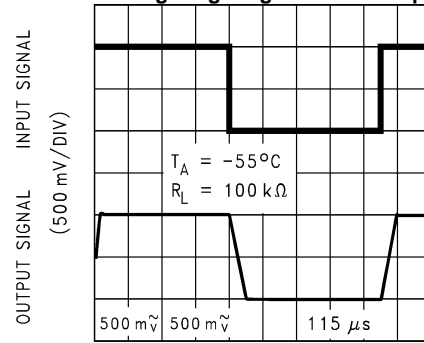
$V_S = +5V$, Single Supply, $T_A = 25^\circ C$ unless otherwise specified

Non-Inverting Large Signal Pulse Response



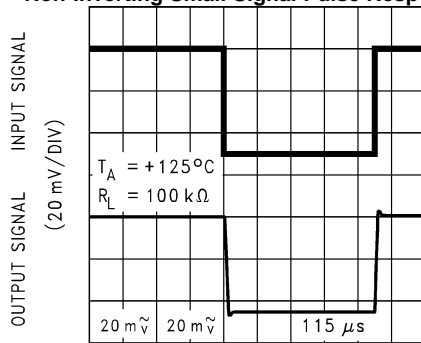
TIME (115 μs /DIV)
Figure 22.

Non-Inverting Large Signal Pulse Response



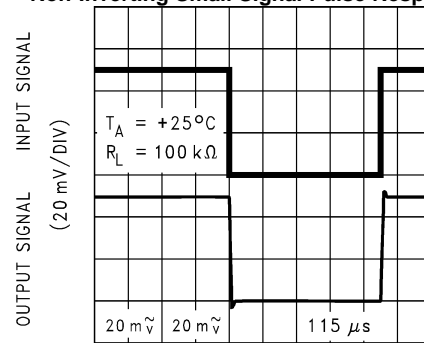
TIME (115 μs /DIV)
Figure 23.

Non-Inverting Small Signal Pulse Response



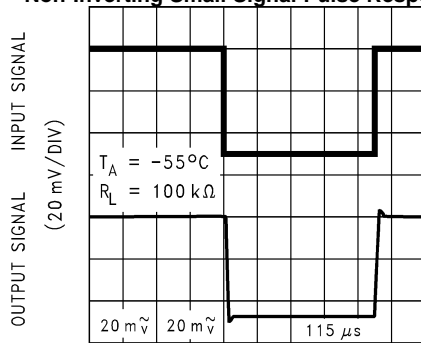
TIME (115 μs /DIV)
Figure 24.

Non-Inverting Small Signal Pulse Response



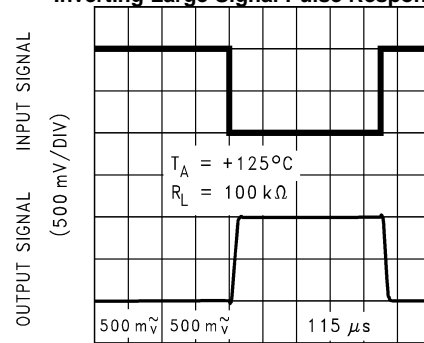
TIME (115 μs /DIV)
Figure 25.

Non-Inverting Small Signal Pulse Response



TIME (115 μs /DIV)
Figure 26.

Inverting Large Signal Pulse Response

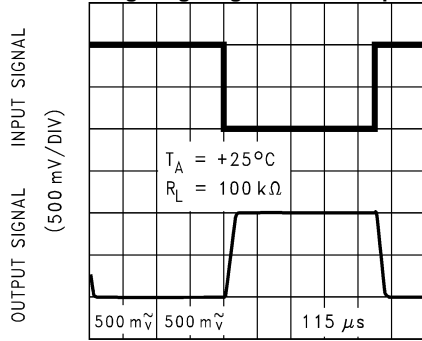


TIME (115 μs /DIV)
Figure 27.

Typical Performance Characteristics (continued)

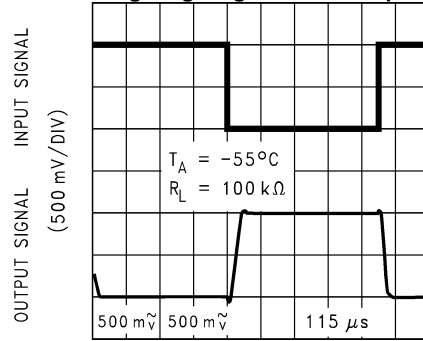
$V_S = +5V$, Single Supply, $T_A = 25^\circ C$ unless otherwise specified

Inverting Large Signal Pulse Response



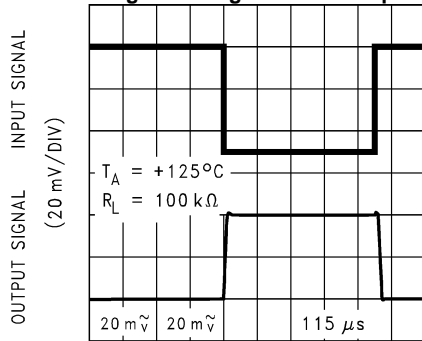
TIME (115 μs /DIV)
Figure 28.

Inverting Large Signal Pulse Response



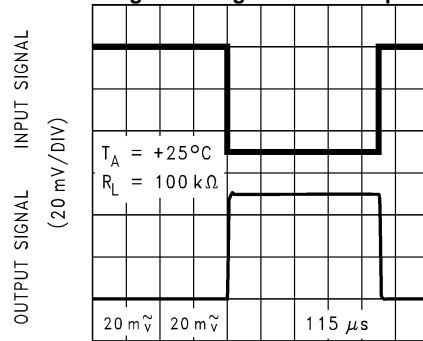
TIME (115 μs /DIV)
Figure 29.

Inverting Small Signal Pulse Response



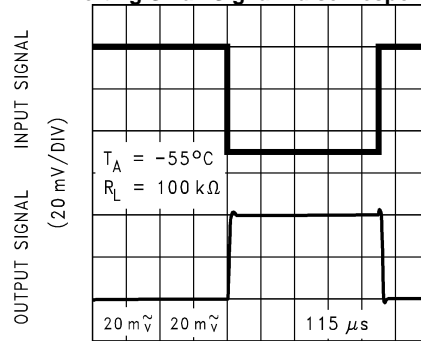
TIME (115 μs /DIV)
Figure 30.

Inverting Small Signal Pulse Response



TIME (115 μs /DIV)
Figure 31.

Inverting Small Signal Pulse Response



TIME (115 μs /DIV)
Figure 32.

APPLICATION INFORMATION

Input Common-Mode Voltage Range

The LMC6462/4 has a rail-to-rail input common-mode voltage range. [Figure 33](#) shows an input voltage exceeding both supplies with no resulting phase inversion on the output.

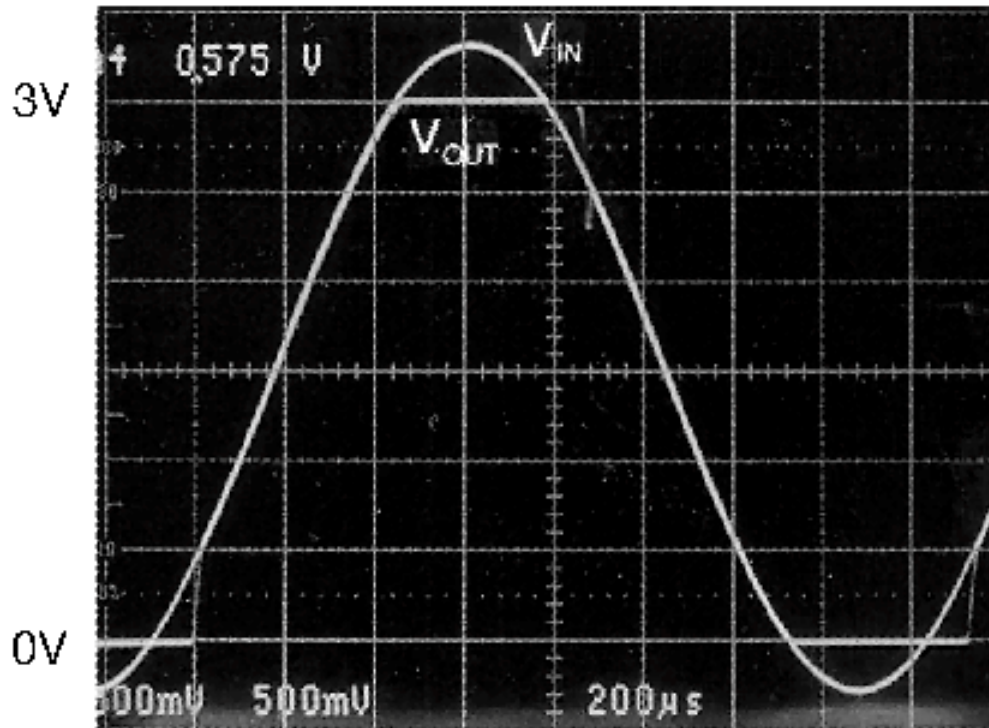


Figure 33. An Input Voltage Signal Exceeds the LMC6462/4 Power Supply Voltage with No Output Phase Inversion

The absolute maximum input voltage at $V^+ = 3V$ is 300 mV beyond either supply rail at room temperature. Voltages greatly exceeding this absolute maximum rating, as in [Figure 34](#), can cause excessive current to flow in or out of the input pins, possibly affecting reliability. The input current can be externally limited to ± 5 mA, with an input resistor, as shown in [Figure 35](#).

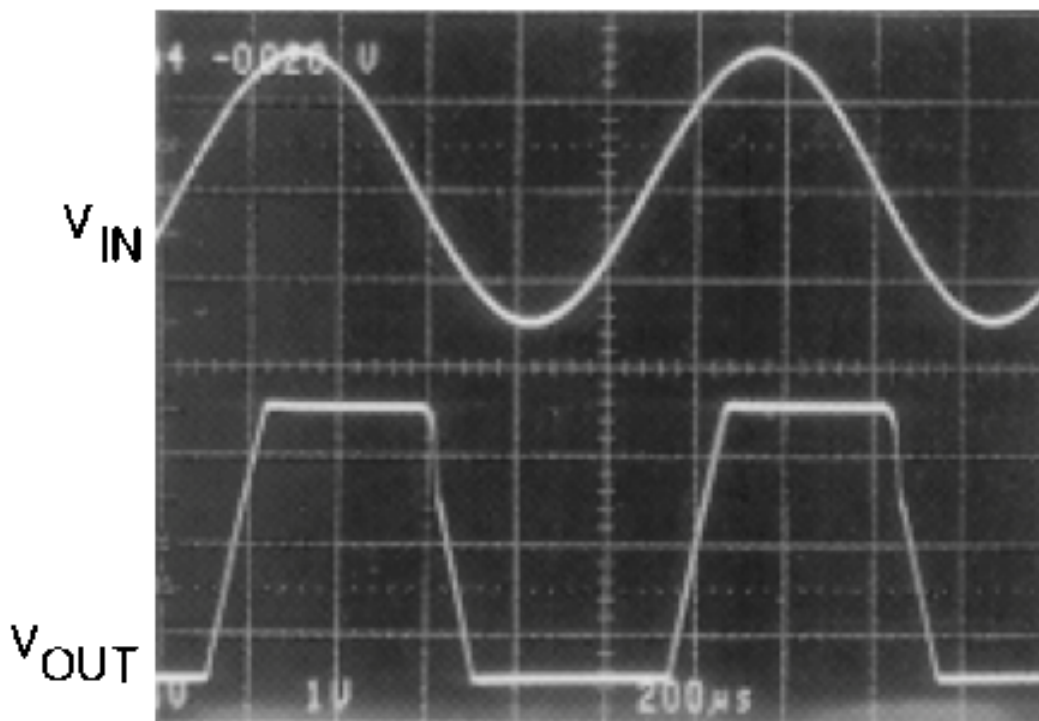


Figure 34. A $\pm 7.5V$ Input Signal Greatly Exceeds the 3V Supply in Figure 35 Causing No Phase Inversion Due to R_I

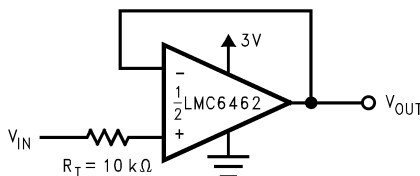


Figure 35. Input Current Protection for Voltages Exceeding the Supply Voltage

Rail-to-Rail Output

The approximated output resistance of the LMC6462/4 is 180Ω sourcing, and 130Ω sinking at $V_S = 3V$, and 110Ω sourcing and 83Ω sinking at $V_S = 5V$. The maximum output swing can be estimated as a function of load using the calculated output resistance.

Capacitive Load Tolerance

The LMC6462/4 can typically drive a 200 pF load with $V_S = 5V$ at unity gain without oscillating. The unity gain follower is the most sensitive configuration to capacitive load. Direct capacitive loading reduces the phase margin of op-amps. The combination of the op-amp's output impedance and the capacitive load induces phase lag. This results in either an underdamped pulse response or oscillation.

Capacitive load compensation can be accomplished using resistive isolation as shown in Figure 36. If there is a resistive component of the load in parallel to the capacitive component, the isolation resistor and the resistive load create a voltage divider at the output. This introduces a DC error at the output.

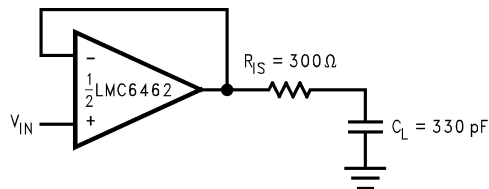


Figure 36. Resistive Isolation of a 300 pF Capacitive Load

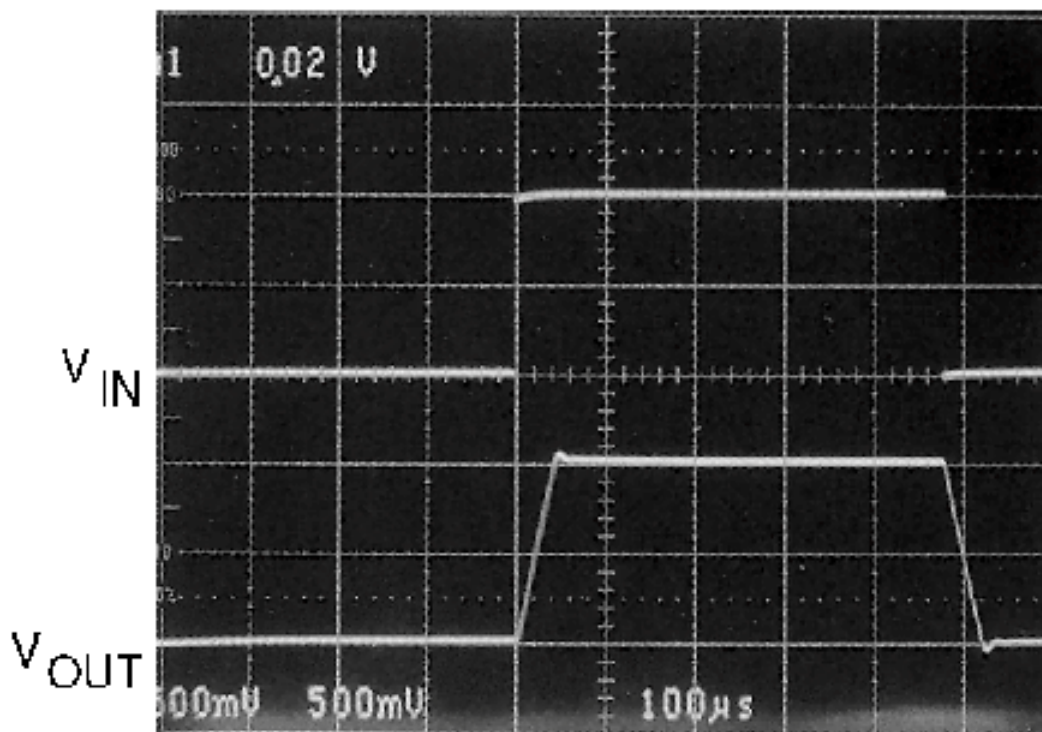


Figure 37. Pulse Response of the LMC6462 Circuit Shown in Figure 36

Figure 37 displays the pulse response of the LMC6462/4 circuit in Figure 36.

Another circuit, shown in Figure 38, is also used to indirectly drive capacitive loads. This circuit is an improvement to the circuit shown in Figure 36 because it provides DC accuracy as well as AC stability. R1 and C1 serve to counteract the loss of phase margin by feeding the high frequency component of the output signal back to the amplifiers inverting input, thereby preserving phase margin in the overall feedback loop. The values of R1 and C1 should be experimentally determined by the system designer for the desired pulse response. Increased capacitive drive is possible by increasing the value of the capacitor in the feedback loop.

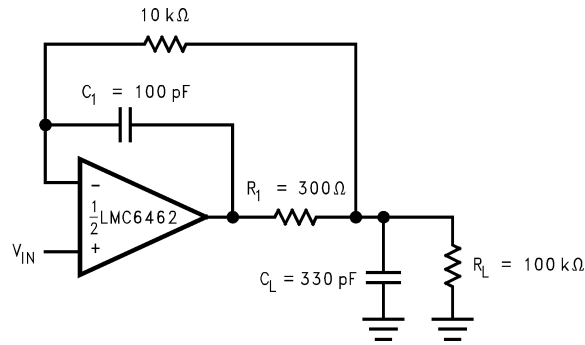


Figure 38. LMC6462 Non-Inverting Amplifier, Compensated to Handle a 300 pF Capacitive and 100 kΩ Resistive Load

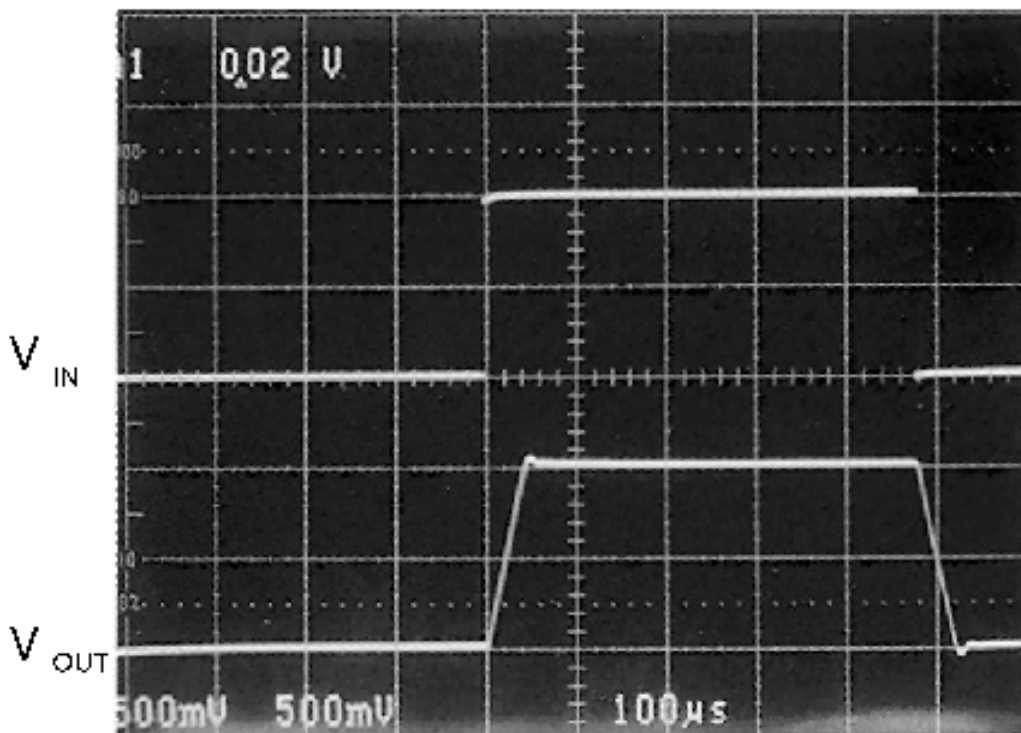


Figure 39. Pulse Response of LMC6462 Circuit in Figure 38

The pulse response of the circuit shown in Figure 38 is shown in Figure 39

Compensating for Input Capacitance

It is quite common to use large values of feedback resistance with amplifiers that have ultra-low input current, like the LMC6462/4. Large feedback resistors can react with small values of input capacitance due to transducers, photodiodes, and circuits board parasitics to reduce phase margins.

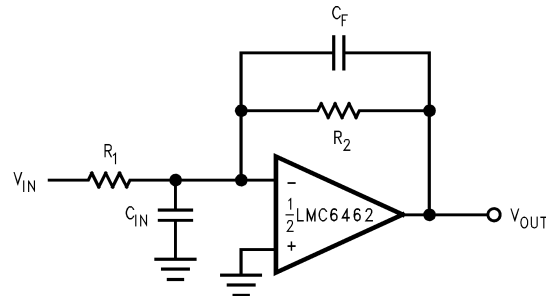


Figure 40. Canceling the Effect of Input Capacitance

The effect of input capacitance can be compensated for by adding a feedback capacitor. The feedback capacitor (as in Figure 40), C_F, is first estimated by:

$$\frac{1}{2\pi R_1 C_{IN}} \geq \frac{1}{2\pi R_2 C_F} \quad (1)$$

or

$$R_1 C_{IN} \leq R_2 C_F \quad (2)$$

which typically provides significant overcompensation.

Printed circuit board stray capacitance may be larger or smaller than that of a breadboard, so the actual optimum value for C_F may be different. The values of C_F should be checked on the actual circuit. (Refer to the LMC660 quad CMOS amplifier data sheet for a more detailed discussion.)

Offset Voltage Adjustment

Offset voltage adjustment circuits are illustrated in Figure 41 and Figure 42. Large value resistances and potentiometers are used to reduce power consumption while providing typically ±2.5 mV of adjustment range, referred to the input, for both configurations with V_S = ±5V.

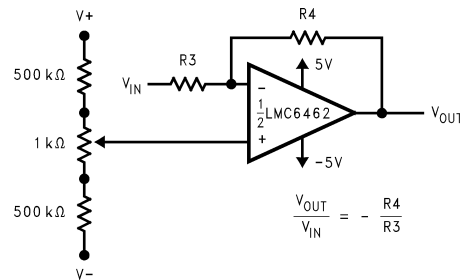


Figure 41. Inverting Configuration Offset Voltage Adjustment

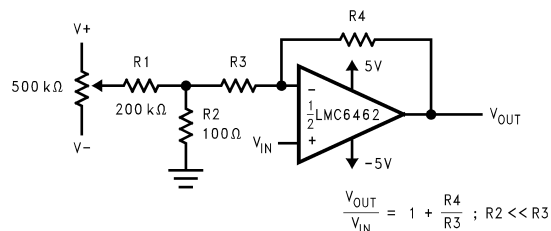


Figure 42. Non-Inverting Configuration Offset Voltage Adjustment

SPICE Macromodel

A Spice macromodel is available for the LMC6462/4. This model includes a simulation of:

- Input common-mode voltage range

- Frequency and transient response
- GBW dependence on loading conditions
- Quiescent and dynamic supply current
- Output swing dependence on loading conditions

and many more characteristics as listed on the macromodel disk.

Contact the Texas Instruments Customer Response Center to obtain an operational amplifier Spice model library disk

Printed-Circuit-Board Layout for High-Impedance Work

It is generally recognized that any circuit which must operate with less than 1000 pA of leakage current requires special layout of the PC board. When one wishes to take advantage of the ultra-low input current of the LMC6462/4, typically 150 fA, it is essential to have an excellent layout. Fortunately, the techniques of obtaining low leakages are quite simple. First, the user must not ignore the surface leakage of the PC board, even though it may sometimes appear acceptably low, because under conditions of high humidity or dust or contamination, the surface leakage will be appreciable.

To minimize the effect of any surface leakage, lay out a ring of foil completely surrounding the LMC6462's inputs and the terminals of capacitors, diodes, conductors, resistors, relay terminals, etc. connected to the op-amp's inputs, as in [Figure 43](#). To have a significant effect, guard rings should be placed in both the top and bottom of the PC board. This PC foil must then be connected to a voltage which is at the same voltage as the amplifier inputs, since no leakage current can flow between two points at the same potential. For example, a PC board trace-to-pad resistance of $10^{12}\Omega$, which is normally considered a very large resistance, could leak 5 pA if the trace were a 5V bus adjacent to the pad of the input. This would cause a 30 times degradation from the LMC6462/4's actual performance. However, if a guard ring is held within 5 mV of the inputs, then even a resistance of $10^{11}\Omega$ would cause only 0.05 pA of leakage current. See [Figure 44](#) through [Figure 46](#) for typical connections of guard rings for standard op-amp configurations.

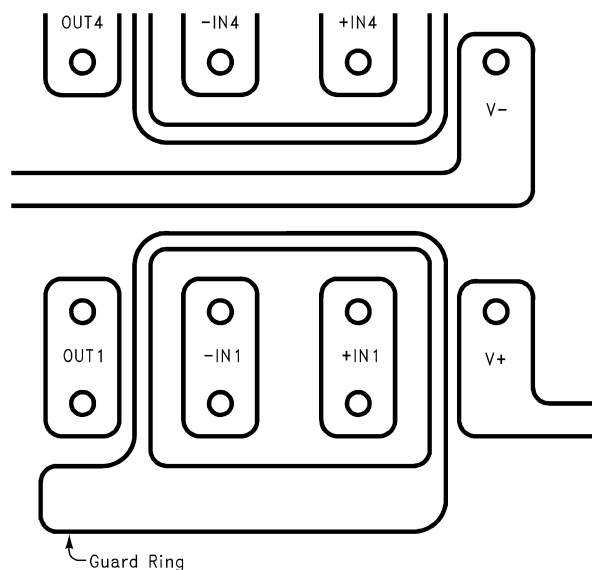


Figure 43. Example of Guard Ring in P.C. Board Layout

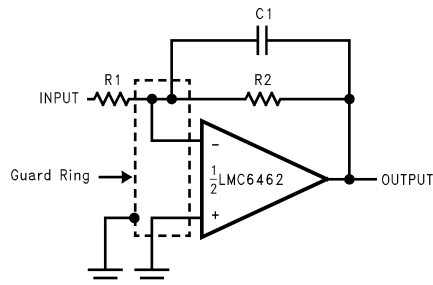


Figure 44. Typical Connections of Guard Rings – Inverting Amplifier

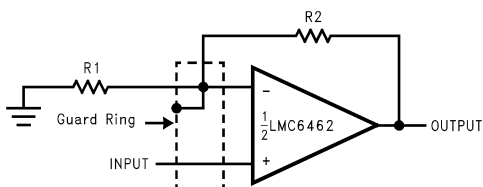


Figure 45. Typical Connections of Guard Rings – Non-Inverting Amplifier

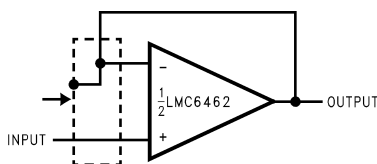
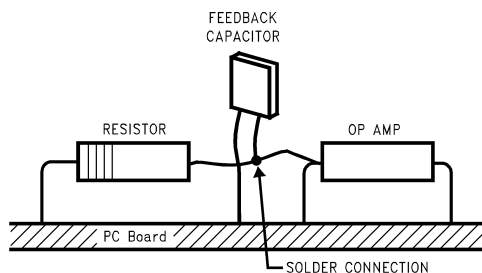


Figure 46. Typical Connections of Guard Rings – Follower

The designer should be aware that when it is inappropriate to lay out a PC board for the sake of just a few circuits, there is another technique which is even better than a guard ring on a PC board: Don't insert the amplifier's input pin into the board at all, but bend it up in the air and use only air as an insulator. Air is an excellent insulator. In this case you may have to forego some of the advantages of PC board construction, but the advantages are sometimes well worth the effort of using point-to-point up-in-the-air wiring. See Figure 47.



(Input pins are lifted out of PC board and soldered directly to components. All other pins connected to PC board.)

Figure 47. Air Wiring

Instrumentation Circuits

The LMC6464 has the high input impedance, large common-mode range and high CMRR needed for designing instrumentation circuits. Instrumentation circuits designed with the LMC6464 can reject a larger range of common-mode signals than most in-amps. This makes instrumentation circuits designed with the LMC6464 an excellent choice for noisy or industrial environments. Other applications that benefit from these features include analytic medical instruments, magnetic field detectors, gas detectors, and silicon-based transducers.

A small valued potentiometer is used in series with R_G to set the differential gain of the three op-amp instrumentation circuit in Figure 48. This combination is used instead of one large valued potentiometer to increase gain trim accuracy and reduce error due to vibration.

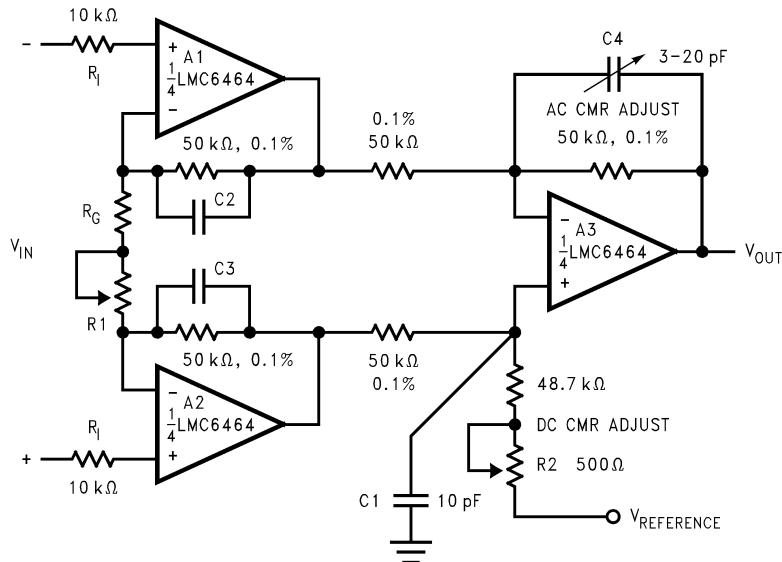


Figure 48. Low Power Three Op-Amp Instrumentation Amplifier

A two op-amp instrumentation amplifier designed for a gain of 100 is shown in Figure 49. Low sensitivity trimming is made for offset voltage, CMRR and gain. Low cost and low power consumption are the main advantages of this two op-amp circuit.

Higher frequency and larger common-mode range applications are best facilitated by a three op-amp instrumentation amplifier.

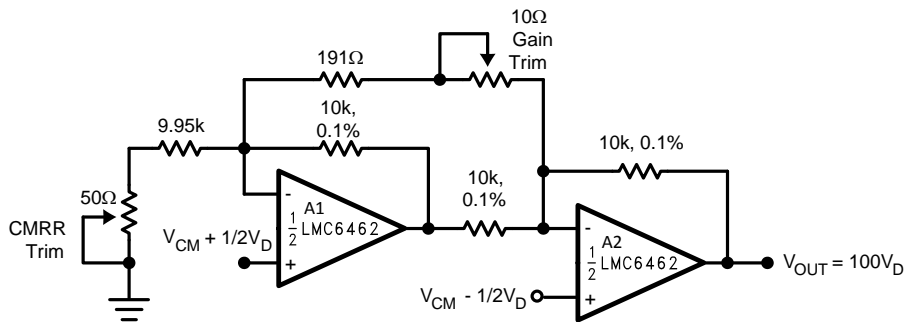


Figure 49. Low-Power Two-Op-Amp Instrumentation Amplifier

TYPICAL SINGLE-SUPPLY APPLICATIONS

Transducer Interface Circuits

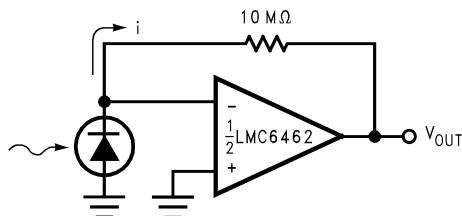


Figure 50. Photo Detector Circuit

Photocells can be used in portable light measuring instruments. The LMC6462, which can be operated off a battery, is an excellent choice for this circuit because of its very low input current and offset voltage.

LMC6462 as a Comparator

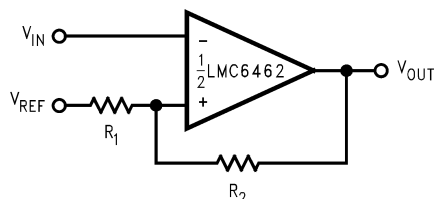


Figure 51. Comparator with Hysteresis

Figure 51 shows the application of the LMC6462 as a comparator. The hysteresis is determined by the ratio of the two resistors. The LMC6462 can thus be used as a micropower comparator, in applications where the quiescent current is an important parameter.

Half-Wave and Full-Wave Rectifiers

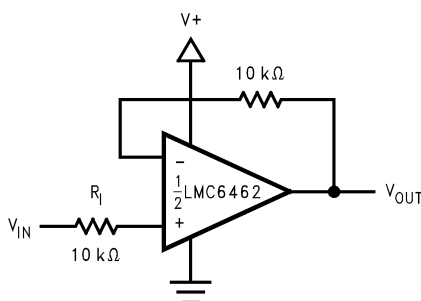


Figure 52. Half-Wave Rectifier with Input Current Protection (R_1)

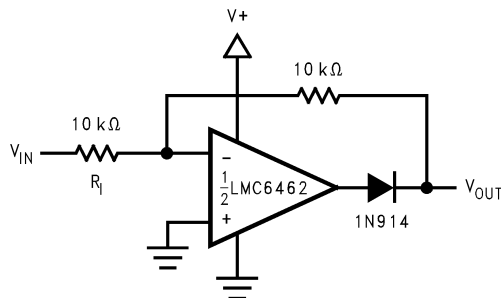


Figure 53. Full-Wave Rectifier with Input Current Protection (R_1)

In Figure 52 Figure 53, R_1 limits current into the amplifier since excess current can be caused by the input voltage exceeding the supply voltage.

Precision Current Source

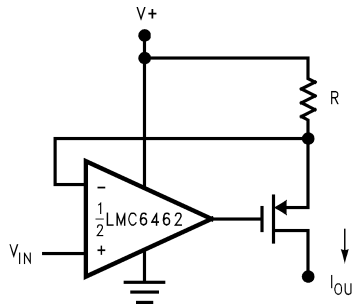


Figure 54. Precision Current Source

The output current I_{OUT} is given by:

$$I_{OUT} = \left(\frac{V^+ - V_{IN}}{R} \right) \tag{3}$$

Oscillators

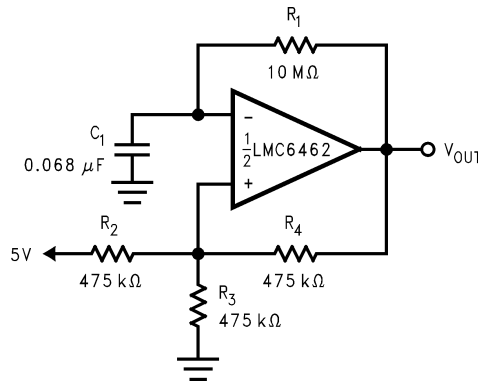


Figure 55. 1 Hz Square-Wave Oscillator

For single supply 5V operation, the output of the circuit will swing from 0V to 5V. The voltage divider set up R_2 , R_3 and R_4 will cause the non-inverting input of the LMC6462 to move from 1.67V ($\frac{1}{3}$ of 5V) to 3.33V ($\frac{2}{3}$ of 5V). This voltage behaves as the threshold voltage.

R_1 and C_1 determine the time constant of the circuit. The frequency of oscillation, f_{OSC} is

$$\left(\frac{1}{2\Delta t} \right) \tag{4}$$

where Δt is the time the amplifier input takes to move from 1.67V to 3.33V. The calculations are shown below.

$$1.67 = 5 \left(1 - e^{-\frac{t_1}{\tau}} \right) \tag{5}$$

where $\tau = RC = 0.68$ seconds

$$\rightarrow t_1 = 0.27 \text{ seconds.}$$

and

$$3.33 = 5 \left(1 - e^{-\frac{t_2}{\tau}} \right) \tag{6}$$

$$\rightarrow t_2 = 0.75 \text{ seconds}$$

Then,

$$f_{osc} = \left(\frac{1}{2\Delta t} \right) \tag{7}$$

$$= \frac{1}{2(0.75 - 0.27)} \tag{8}$$

= 1 Hz

Low Frequency Null

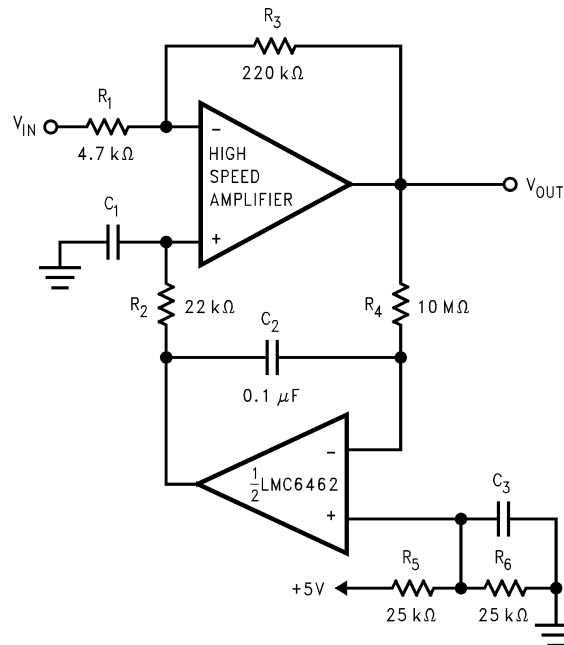


Figure 56. High Gain Amplifier with Low Frequency Null

Output offset voltage is the error introduced in the output voltage due to the inherent input offset voltage V_{OS} , of an amplifier.

Output Offset Voltage = (Input Offset Voltage) (Gain)

In the above configuration, the resistors R_5 and R_6 determine the nominal voltage around which the input signal, V_{IN} should be symmetrical. The high frequency component of the input signal V_{IN} will be unaffected while the low frequency component will be nulled since the DC level of the output will be the input offset voltage of the LMC6462 plus the bias voltage. This implies that the output offset voltage due to the top amplifier will be eliminated.

REVISION HISTORY

Changes from Revision C (March 2013) to Revision D	Page
• Changed layout of National Data Sheet to TI format	21

PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
LMC6462AIM	NRND	SOIC	D	8	95	TBD	Call TI	Call TI	-40 to 85	LMC64 62AIM	
LMC6462AIM/NOPB	ACTIVE	SOIC	D	8	95	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC64 62AIM	Samples
LMC6462AIMX/NOPB	ACTIVE	SOIC	D	8	2500	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC64 62AIM	Samples
LMC6462AIN/NOPB	ACTIVE	PDIP	P	8	40	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM	-40 to 85	LMC6462 AIN	Samples
LMC6462B-MDC	ACTIVE	DIESALE	Y	0	324	Green (RoHS & no Sb/Br)	Call TI	Level-1-NA-UNLIM	-40 to 85		Samples
LMC6462BIM/NOPB	ACTIVE	SOIC	D	8	95	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC64 62BIM	Samples
LMC6462BIMX/NOPB	ACTIVE	SOIC	D	8	2500	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC64 62BIM	Samples
LMC6462BIN/NOPB	ACTIVE	PDIP	P	8	40	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM	-40 to 85	LMC6462 BIN	Samples
LMC6464AIM	NRND	SOIC	D	14	55	TBD	Call TI	Call TI	-40 to 85	LMC6464 AIM	
LMC6464AIM/NOPB	ACTIVE	SOIC	D	14	55	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC6464 AIM	Samples
LMC6464AIMX	NRND	SOIC	D	14	2500	TBD	Call TI	Call TI	-40 to 85	LMC6464 AIM	
LMC6464AIMX/NOPB	ACTIVE	SOIC	D	14	2500	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC6464 AIM	Samples
LMC6464BIM	NRND	SOIC	D	14	55	TBD	Call TI	Call TI	-40 to 85	LMC6464 BIM	
LMC6464BIM/NOPB	ACTIVE	SOIC	D	14	55	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC6464 BIM	Samples
LMC6464BIMX	NRND	SOIC	D	14	2500	TBD	Call TI	Call TI	-40 to 85	LMC6464 BIM	
LMC6464BIMX/NOPB	ACTIVE	SOIC	D	14	2500	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 85	LMC6464 BIM	Samples
LMC6464BIN/NOPB	ACTIVE	PDIP	NFF	14	25	Green (RoHS & no Sb/Br)	CU SN	Level-1-NA-UNLIM	-40 to 85	LMC6464BIN	Samples

(1) The marketing status values are defined as follows:

ACTIVE: Product device recommended for new designs.

LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

PREVIEW: Device has been announced but is not in production. Samples may or may not be available.

OBSOLETE: TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

TBD: The Pb-Free/Green conversion plan has not been defined.

Pb-Free (RoHS): TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

Pb-Free (RoHS Exempt): This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

Green (RoHS & no Sb/Br): TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LMC6462AIMX/NOPB	SOIC	D	8	2500	330.0	12.4	6.5	5.4	2.0	8.0	12.0	Q1
LMC6462BIMX/NOPB	SOIC	D	8	2500	330.0	12.4	6.5	5.4	2.0	8.0	12.0	Q1
LMC6464AIMX	SOIC	D	14	2500	330.0	16.4	6.5	9.35	2.3	8.0	16.0	Q1
LMC6464AIMX/NOPB	SOIC	D	14	2500	330.0	16.4	6.5	9.35	2.3	8.0	16.0	Q1
LMC6464BIMX	SOIC	D	14	2500	330.0	16.4	6.5	9.35	2.3	8.0	16.0	Q1
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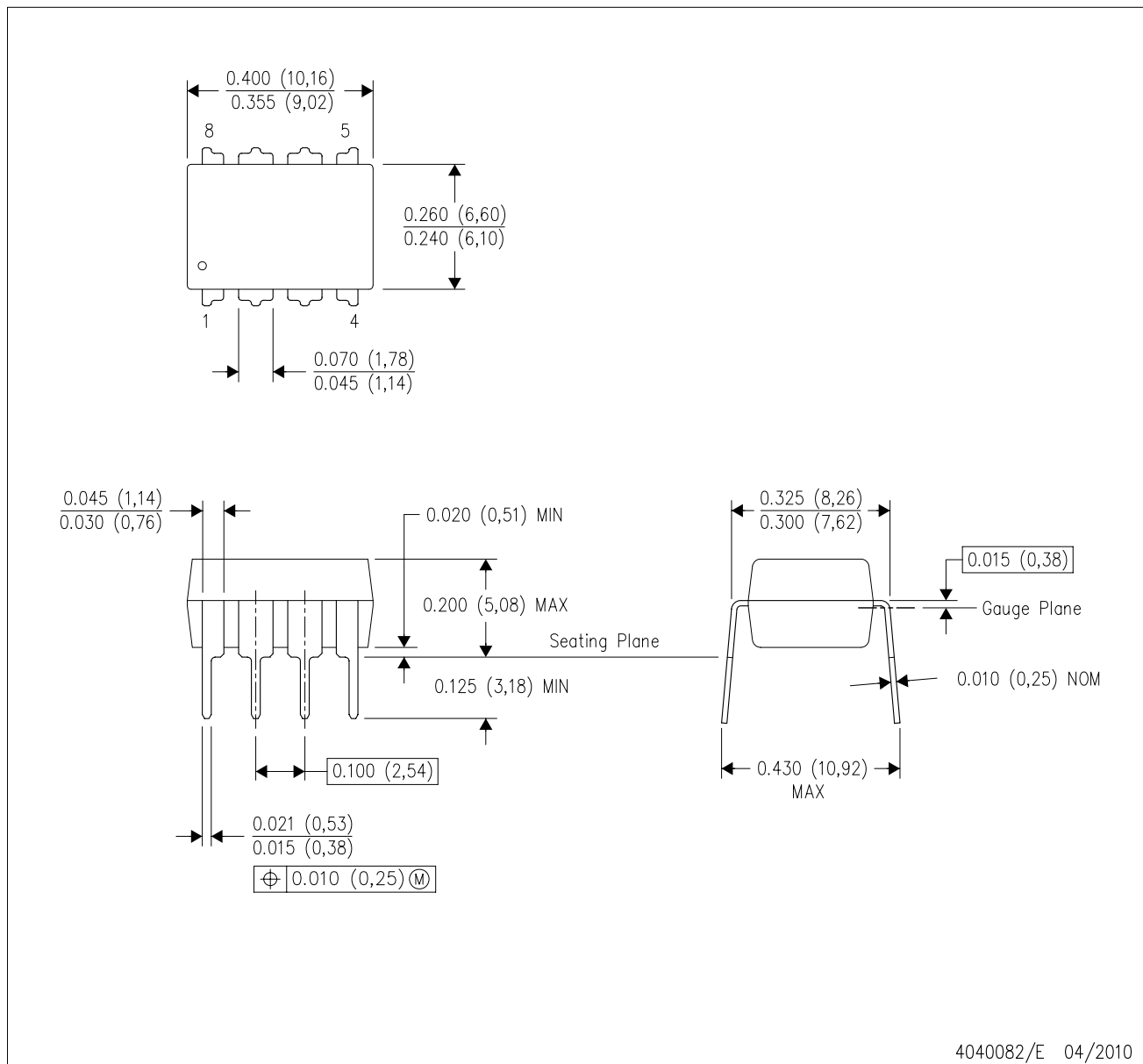
TAPE AND REEL BOX DIMENSIONS


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LMC6462AIMX/NOPB	SOIC	D	8	2500	367.0	367.0	35.0
LMC6462BIMX/NOPB	SOIC	D	8	2500	367.0	367.0	35.0
LMC6464AIMX	SOIC	D	14	2500	367.0	367.0	35.0
LMC6464AIMX/NOPB	SOIC	D	14	2500	367.0	367.0	35.0
LMC6464BIMX	SOIC	D	14	2500	367.0	367.0	35.0
LMC6464BIMX/NOPB	SOIC	D	14	2500	367.0	367.0	35.0

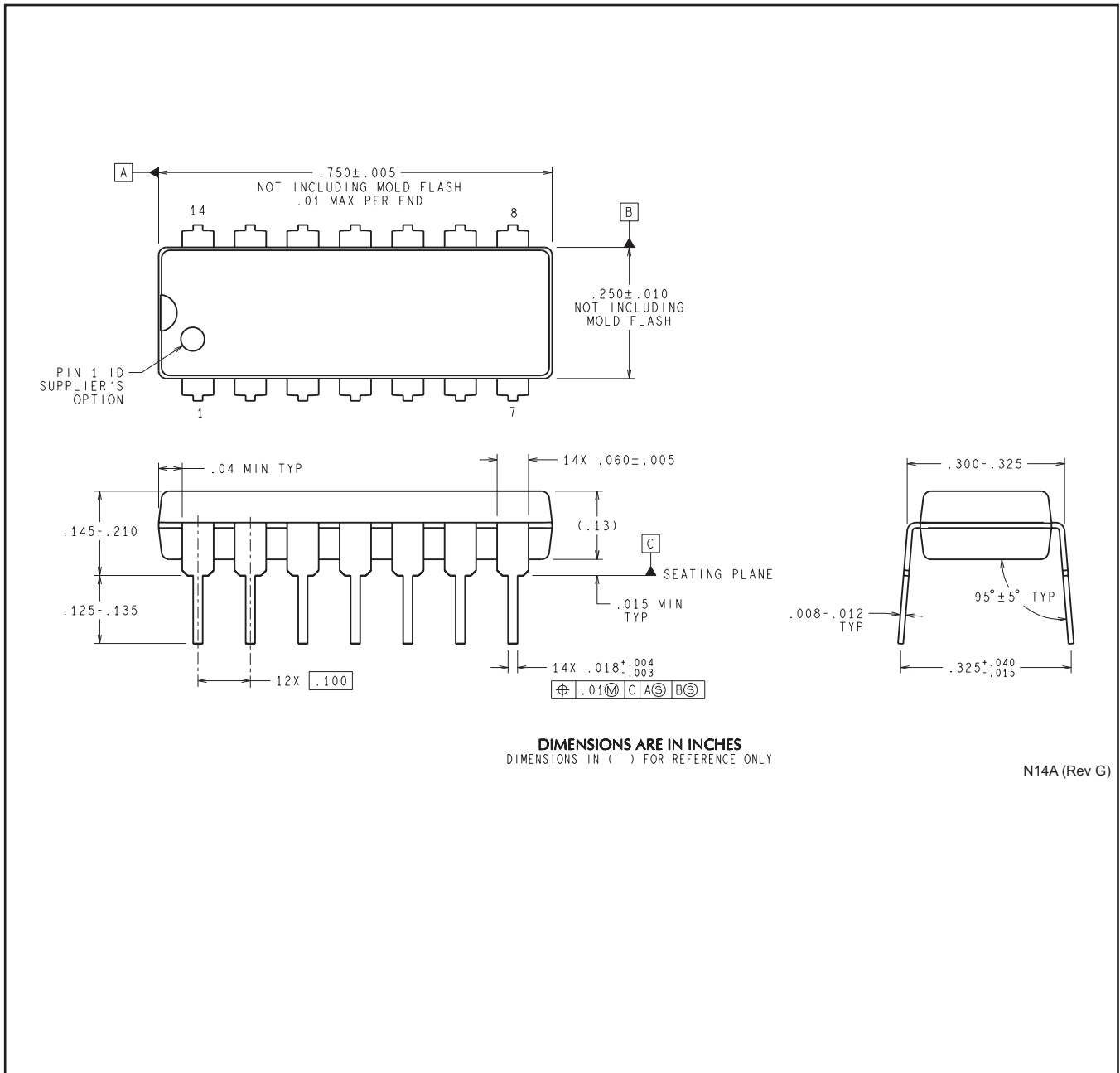
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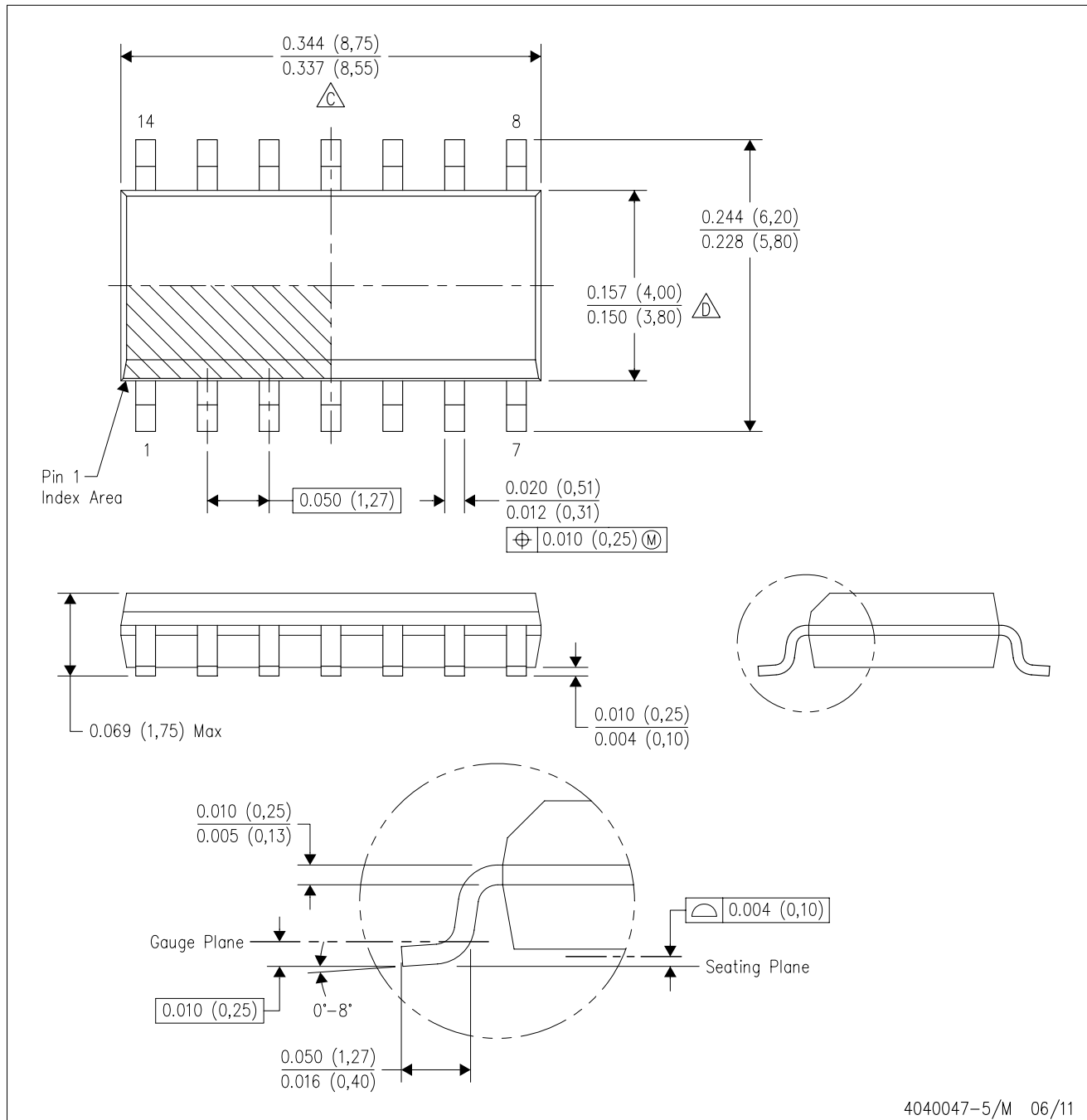




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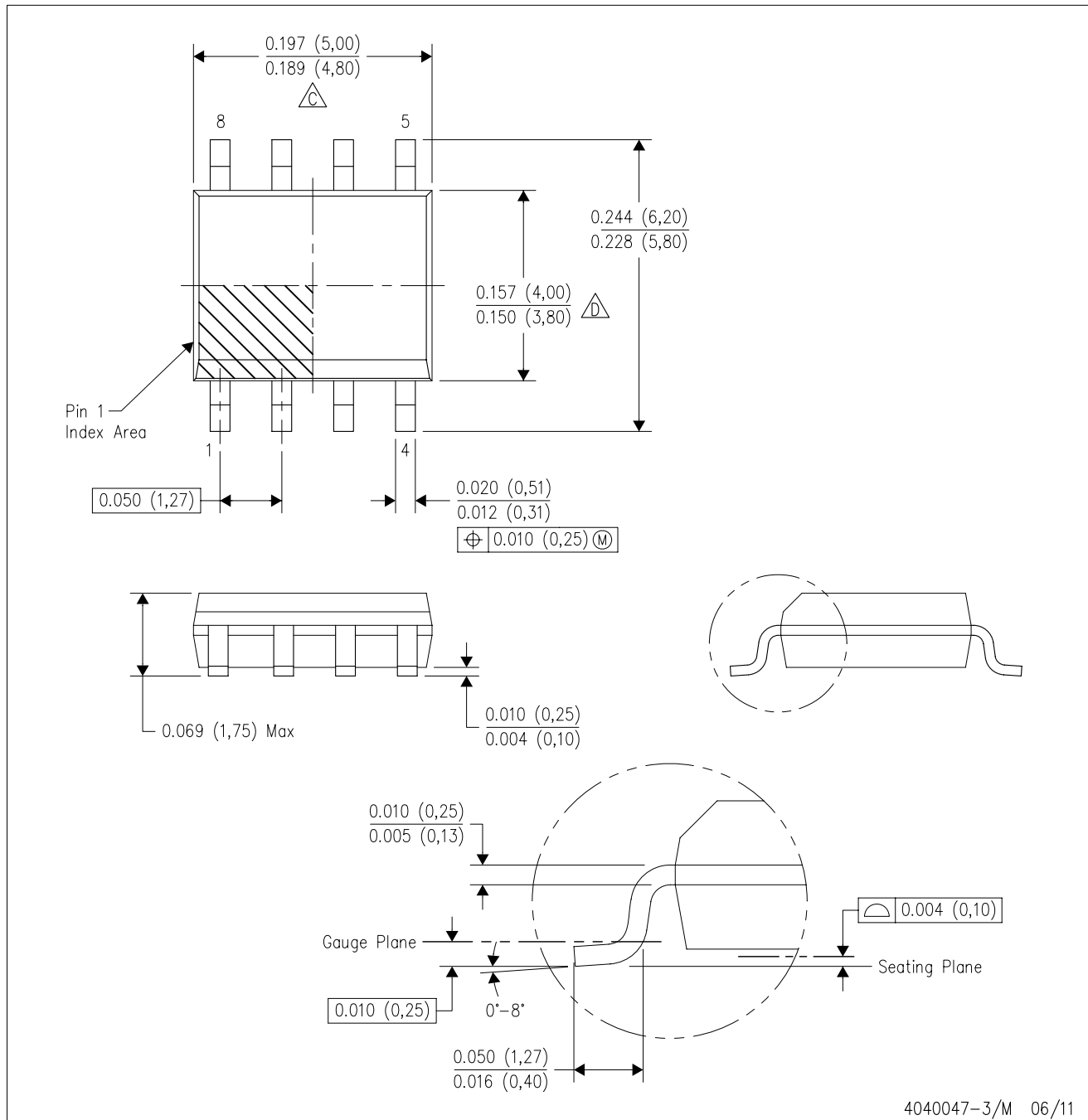
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 -  Body width does not include interlead flash. Interlead flash shall not exceed 0.017 (0,43) each side.
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